

Research Article

Novel Precoded Relay-Assisted Algorithm for Cellular Systems

Sara Teodoro, Adão Silva, João M. Gil, and Atilio Gameiro

Instituto de Telecomunicações, Universidade de Aveiro, 3810-193 Aveiro, Portugal

Correspondence should be addressed to Sara Teodoro, steodoro@av.it.pt

Received 14 July 2010; Accepted 11 November 2010

Academic Editor: Richard Kozick

Copyright © 2010 Sara Teodoro et al. This is an open access article distributed under the Creative Commons Attribution License, which permits unrestricted use, distribution, and reproduction in any medium, provided the original work is properly cited.

Cooperative schemes are promising solutions for cellular wireless systems to improve system fairness, extend coverage and increase capacity. The use of relays is of significant interest to allow radio access in situations where a direct path is not available or has poor quality. A data precoded relay-assisted scheme is proposed for a system cooperating with 2 relays, each equipped with either a single antenna or 2-antenna array. However, because of the half-duplex constraint at the relays, relaying-assisted transmission would require the use of a higher order constellation than in the case when a continuous link is available from the BS to the UT. This would imply a penalty in the power efficiency. The simple precoding scheme proposed exploits the relation between QPSK and 16-QAM, by alternately transmitting through the 2 relays, achieving full diversity, while significantly reducing power penalty. Analysis of the pairwise error probability of the proposed algorithm with a single antenna in each relay is derived and confirmed with numerical results. We show the performance improvements of the precoded scheme, relatively to equivalent distributed SFBC scheme employing 16-QAM, for several channel quality scenarios.

1. Introduction

Multiple-input, multiple-output (MIMO) wireless communications are effective in mitigating channel fading, thus improving the cellular system capacity [1]. However, there is significant correlation between channels in some environments, and using an antenna array at the user terminal (UT) may not be feasible due to size, cost, and hardware limitations. Cooperative systems are promising solutions for wireless systems to overcome such limitations, when the direct link does not have good transmission conditions [2]. It can be achieved through cooperation of terminals (either dedicated or user terminals acting as relays), which share their antennas and thereby create a virtual antenna array (VAA) or a virtual MIMO (VMIMO) system [3]. These allow single antenna devices to benefit from spatial diversity without the need for colocated additional physical antenna arrays.

Several cooperative diversity protocols have been proposed and analysed to demonstrate the potential benefits of cooperation [4, 5]. In [6], a theoretical diversity-multiplexing trade-off study is presented regarding a cooperative system with 1 and 2 antennas in a single-relay scheme. Furthermore, in [7] the Rayleigh performance of

a single-relay cooperative scenario with multiple-antenna nodes is investigated, deriving pairwise error probability (PEP) expressions. In order to get higher diversity orders, one can also consider the use of multiple-relay nodes [8]. However, increasing the number of relays reduces the bandwidth efficiency of the system, as the source uses only a fraction of the total available degrees of freedom to transmit the information.

In [9], the idea of space-time coding devised for point-to-point colocated multiple antenna systems is applied for a wireless relay network with single antenna nodes and PEP of such a scheme is derived. The authors show that in a relay network with a single source, a single destination with R single antenna relays, distributed space-time coding (DSTC) asymptotically approaches the diversity of a colocated multiple antenna system with R transmit antennas and one receiving antenna. More recently, in [10], distributed orthogonal space-time block codes (DOSTBCs) achieving single-symbol decodability have been introduced for cooperative networks. The authors considered a special class of these codes (row monomial DOSTBCs), deriving upper-bounds on the maximum symbol-rate. In [11], single-symbol decodable (SSD) DSTBCs have been studied when the relay nodes are assumed to know the corresponding

channel phase information. An upper bound on the symbol rate for such a set up is shown to be one half of the rate of the direct link transmission when this link is available, which is independent of the number of relays. In [12], a semi-orthogonal precoded DSTBC was proposed, wherein the source performs precoding on the information symbols before transmitting it to all the relays. Several relays are considered all equipped with a single antenna. A systematic construction of these codes is presented for more than 3 relays and the constructed codes are shown to have higher rates than those of DOSTBCs. Although achieving full diversity, these distributed orthogonal algorithms cannot achieve full spectral efficiency, since they use 2 phases for transmission. For this reason, these cooperative systems achieve half of the bandwidth efficiency of the equivalent non-cooperative systems.

Other works were developed with the objective of increasing capacity or diversity order of cooperative systems, using non-orthogonal protocols for cooperative systems with 2 or more relays, as in [13, 14]. In [13] a generalised non-orthogonal amplify-and-forward protocol is proposed with a low decoder complexity, achieving better error performances than in [9], depending on the coding. In [14] coding strategies are studied for non-orthogonal cooperative channels, using one or more designed space-time precoders, in a protocol where inter-relay communication is allowed, but again having no full spectral efficiency. In these non-orthogonal algorithms, transmission via an existing direct path is required. Thus, in situations with poor direct link conditions, performance is significantly degraded and in case of outage of one relay some information can be lost.

Further along the development of cooperative systems, some relay precoder designs were also proposed, however with different goals [15, 16]. In [15], the precoder maximizes the capacity between the source and destination nodes in a non-regenerative relay system, with a single relay node, considering all the nodes with multiple antennas. In [16], MIMO relay provides robustness against imperfect channel state information (CSI), for a multipoint-to-multipoint communication through the use of a relay precoder design.

Our previous work included a distributed space-frequency block coding (SFBC) scheme, designed for orthogonal frequency-division multiplexing-based cellular systems, requiring a direct path [17]. We have thereby considered the use of an antenna array at the base station (BS) and a single antenna at both the UT and relay node (RN). We observed better performances with the cooperative systems against the non-cooperative, when one has better link quality in the first hop to the relay than the direct link. However, as the other cooperative systems recently proposed, this scheme has also half of the spectral efficiency of the respective non-cooperative system. Because of the half-duplex constraint at the relays, transmission of a data rate equivalent to that of a modulation technique with m bits per symbol in the case the direct link would be available from the BS to the UT would require the use of a constellation with $2m$ bits per symbol. This would imply a penalty in the power efficiency.

The aim of this paper is to propose a novel data-precoded relay-assisted (RA) algorithm, which can achieve

full spatial diversity, obtaining a coding gain in comparison with the equivalent distributed SFBCs scheme, maintaining the same spectral efficiency of the non-cooperative system. Two RNs are used for cooperation, equipped with either 1 or 2 antennas. The simple precoding scheme proposed exploits the relation between QPSK and 16-QAM, by alternately transmitting through the 2 relays, achieving full diversity, while significantly reducing power penalty. Also there is no need to transmit through the direct link, in alternative to the non-orthogonal algorithms proposed previously. This is beneficial for most scenarios, since the direct link is usually strongly affected by path loss or shadowing. In this algorithm, we perform precoding of the data symbols prior to transmission and posterior decoding at the UT by using Viterbi algorithm [18]. Analysis of the pairwise error probability of the proposed algorithm with a single antenna in each relay is derived and confirmed with numerical results.

The remainder of the paper is organized as follows: in Section 2, a general description of the system model considered is presented; we then describe the proposed algorithm and derive the main link equations as well as compare the proposed scheme with the equivalent distributed SFBC system, for both cases of 1 and 2 antennas at relays, in Section 3; also, pairwise error probability derivation and diversity analysis is made for the proposed algorithm with 1 antenna at each relay, in the same section; then, in Section 4, we present the comparison between theoretical and simulation results, and the performance of the precoded algorithm is assessed and compared with the reference cooperative and non-cooperative systems; finally, main conclusions are pointed out in Section 5.

2. System Model

The system considered consists of 1 BS, 1 UT, and 2 RNs. BS is equipped with K antennas and the UT with a single antenna, whereas RNs have M antennas each, with $M \in \{1, 2\}$, being referred as RA $K \times M \times 1$ (Figure 1). As we consider error-free BS-RN channels, the number of antennas at the base station is irrelevant. However, in practical systems using multiple antennas at the BS increases the probability of finding relays providing good BS-RN quality links. Channels are modelled by Rayleigh flat-fading channels and are represented by $h_{br,qlm}$ for the link formed between the q th antenna of BS and the m th antenna of RN $_l$, and by $h_{ru,lm}$ for the link between the m th antenna of RN $_l$ and UT, with $q = 1, \dots, K$, $l = 1, 2$, and $m = 1, \dots, M$.

The fact that we have two independent paths from the relays to the destination allows us to achieve diversity, assuming error-free links from source to relays. We consider the case that the relays are half-duplex; that is, they cannot transmit and receive at the same time. Considering the half-duplex nature, we may have several options.

The relay nodes are allowed to simultaneously transmit over the same channel by emulating a space-frequency code. Concerning this scheme with single antenna relays, RA $K \times 1 \times 1$ system, Alamouti coding can be implemented in a distributed fashion by the 2 relay nodes [19]. Assuming now a system with 2 antennas in each relay, the quasi-orthogonal

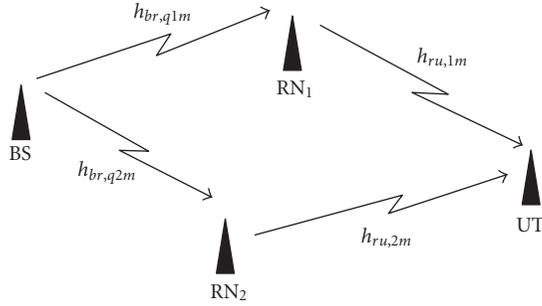


FIGURE 1: System model for the RA scheme with 2 RNs and M antennas at each relay (RA $K \times M \times 1$).

SFBC (QO-SFBC) proposed in [20] can also be implemented in a distributed manner.

Another case occurs when the relays receive and transmit alternately and the source is transmitting continuously, firstly sending the information to the RN_1 and then repeating it to the RN_2 . In this approach, diversity is achieved without need for any extra processing at the relays and using maximum ratio combining at the UT.

In the above two approaches spatial diversity can be achieved, but because of the half-duplex constraints of relays, the information has to be transmitted in half of the time that would be needed in the case of a continuous link available from the source to the destination. This means that, assuming that a modulation scheme carrying m bits per symbol could be used in the case when continuous direct link was available, one would need to switch towards a modulation carrying $2m$ bits per symbol (if the symbol duration was kept identical), for example, going from QPSK to 16-QAM when 2 RNs are available. As a major consequence, increasing modulation order leads to a decrease of power efficiency. However, as we will show in the next sections, the relation between 16-QAM and QPSK defines an inherent trellis structure that can be used to bring the performance closer to the one that would be obtained with the more power efficient modulation scheme.

In another manner, the relays can receive and transmit alternately, while the source is transmitting continuously, according to Figure 2, maintaining spectral efficiency and modulation as compared to the non-cooperative scheme. However, no diversity can be achieved in this case. In order to get both full spectral efficiency and diversity, we propose a novel algorithm where the data symbols are precoded, prior to the source's transmission to the RNs. The data information received and transmitted in each time slot is exemplified in Figure 2, for the case of single antenna RNs (RA Precoded $K \times 1 \times 1$), where s_k is the precoded symbol in time slot k . Precoding is chosen so that diversity can be achieved without the need of exact duplication of the signal. In this cooperative algorithm for the 2-antenna's relays scheme (RA Precoded $K \times 2 \times 1$), the signals transmitted by the 2 antennas are space-frequency encoded using the Alamouti coding, as we can see in Figure 3. In this table the pair of symbols (a, b) represents two symbols transmitted or received in adjacent subcarriers: symbol a

T_s	1	2	3	4	5	...	$2k-1$	$2k$
BS	s_1	s_2	s_3	s_4	s_5		s_{2k-1}	s_{2k}
RN_1	s_1	s_1	s_3	s_3	s_4		s_{2k-2}	s_{2k}
RN_2		s_2	s_2	s_4	s_4		s_{2k-1}	s_{2k-1}
UT		y_2	y_3	y_4	y_5		y_{2k-1}	y_{2k}

FIGURE 2: Transmitted (lighter cells) and received (darker cells) signals corresponding to each node of the RA $K \times 1 \times 1$ scheme with Precoded algorithm.

T_s	$2k-1$	$2k$
BS	$(s_{2k-1}^p; s_{2k-1}^{p+1})$	$(s_{2k}^p; s_{2k}^{p+1})$
RN_{11}	$(s_{2k-1}^p; s_{2k-1}^{p+1})$	$(s_{2k-1}^p; s_{2k-1}^{p+1})$
RN_{12}	$(s_{2k-1}^p; s_{2k-1}^{p+1})$	$(-s_{2k-1}^{p+1*}; s_{2k-1}^{p*})$
RN_{21}	$(s_{2k-2}^p; s_{2k-2}^{p+1})$	$(s_{2k-1}^p; s_{2k-1}^{p+1})$
RN_{22}	$(-s_{2k-2}^{p+1*}; s_{2k-2}^{p*})$	$(s_{2k-1}^p; s_{2k-1}^{p+1})$
UT	$(y_{2k-1}^p; y_{2k-1}^{p+1})$	$(y_{2k}^p; y_{2k}^{p+1})$

FIGURE 3: Transmitted (lighter cells) and received (darker cells) signals corresponding to each node of the RA $K \times 2 \times 1$ scheme with Precoded algorithm.

corresponds to subcarrier p and b to subcarrier $p+1$. The superscript in signals also refers to subcarrier position. Assuming uncorrelated antenna channels, a diversity order of 4 can be achieved.

The rate of the proposed scheme is $N/(N+1)$, where N is the number of symbols transmitted, which is close to 1 for large values of N .

We further assume that each relay node is capable of deciding whether or not it has decoded correctly. If an RN decodes correctly, it will forward the BS data in the second phase; otherwise it remains idle. This can be achieved through the use of cyclic redundancy check codes. This performance can also be approximated by setting a signal-to-noise ratio (SNR) threshold at both RNs; the RN will only forward the source data if the received SNR is larger than that threshold [9].

3. Data-Precoded Algorithm

Let us assume that the source produces a sequence of symbols $\{x_k\}$, each one carrying m information bits. The BS transmitter precodes successive pairs of symbols $\{x_k, x_{k-1}\}$, using a bijective function $F(x_k, x_{k-1})$. The precoded symbols, s_k , are alternately transmitted to the two relays, allowing that each symbol reaches the UT through two independent links. When one of the links fails, the bijectivity allows to recover the original symbols QPSK, as shown in Figure 4.

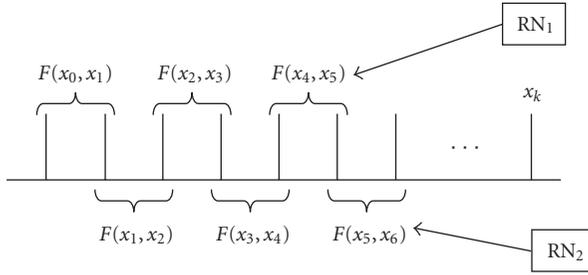


FIGURE 4: Pairs of symbols alternately transmitted to each relay, according to a bijective function $F(x_k, x_{k+1})$.

In the case that original symbols are QPSK, one can use a simple precoding operation that relates QPSK and 16-QAM, obtaining the symbols transmitted by the BS given by

$$s_k = \alpha \left(x_k + \frac{1}{2} x_{k+1} \right), \quad (1)$$

where x_k is the k th QPSK symbol of the original sequence information, with unitary power; α is a normalization factor, so that the average transmitted power is 1, in this case being $\alpha = 2/\sqrt{5}$. From (1), we can easily recognize that each symbol s_k is a 16-QAM symbol. However, the receiver will interpret it as a sum of 2 QPSK symbols, allowing, because of the fact that each QPSK symbol is received through two paths, to bring the performance close to the one that would be achieved if the QPSK symbols were transmitted continuously.

In the proposed precoded algorithm, while BS transmits data continually to the RNs, relays transmit and receive alternately: RN₁ transmits in even time slots, or symbol duration, while RN₂ receives; RN₂ transmits in odd time slots, during the reception period of RN₁ (Figure 2). At the UT, we use the Viterbi decoding algorithm to separate the QPSK data symbols, since it is the optimal decoding method [21]. In the following the signal expressions and methods are presented in detail, separately for each scheme.

3.1. RA Scheme with 1 Antenna at Relays. The received signals at UT, when we have a single-antenna at each relay, in time slots $2k$ and $2k + 1$, are given by

$$\begin{aligned} y_{2k} &= \alpha h_{ru,11,2k} \left(x_{2k-1} + \frac{1}{2} x_{2k} \right) + n_{2k}, \\ y_{2k+1} &= \alpha h_{ru,21,2k+1} \left(x_{2k} + \frac{1}{2} x_{2k+1} \right) + n_{2k+1}, \end{aligned} \quad (2)$$

where $h_{ru,l1,k} = \sqrt{\beta_{l1}} h_{ru,l1,k}^R$ represents the cooperative channel for links RN _{l} → UT; $h_{ru,l1,k}^R$ is the complex flat-fading Rayleigh channel realization for time slot k , with unit average power and β_{l1} represents the long-term channel power; n_{2k+1} and n_{2k+2} are the zero mean complex additive white Gaussian noise samples with variance of σ_n^2 .

It is easy to see that the proposed scheme has a trellis structure for the transmission of the QPSK symbols x_k . As the code is linear, we can assume that symbol $\mathbf{0}$ (algebraically

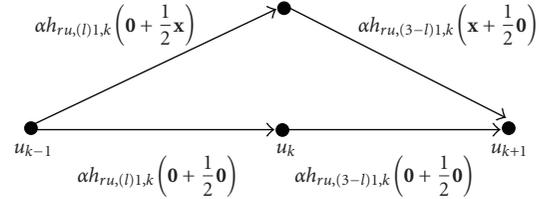


FIGURE 5: Trellis code for RA-Precoded scheme between symbols $\mathbf{0}$ and \mathbf{x} .

as $(0, 0)$) is transmitted. An error event can be recovered in two steps as shown in Figure 5. The distance for the path that erroneously will recover \mathbf{x} instead of $\mathbf{0}$ is given by (3), where $d(\mathbf{0}, \mathbf{x})$ is the distance between the QPSK symbols $\mathbf{0}$ and \mathbf{x} . The minimum distance between two diverging paths is

$$(d^2)_{\text{RA-Prec}} = \alpha^2 d^2(\mathbf{0}, \mathbf{x}) \left(\frac{|h_{ru,l1,k}|^2}{4} + |h_{ru,(3-l)1,k}|^2 \right). \quad (3)$$

As the error events can start at an odd or even time slot, the minimum distance is given by

$$\begin{aligned} (d_{\min}^2)_{\text{RA-Prec}} &= \alpha^2 d_{\min\text{QPSK}}^2 \\ &\times \min \left(\left(\frac{|h_{ru,l1,k}|^2}{4} + |h_{ru,(3-l)1,k}|^2 \right), \right. \\ &\quad \left. \left(|h_{ru,l1,k}|^2 + \frac{|h_{ru,(3-l)1,k}|^2}{4} \right) \right), \end{aligned} \quad (4)$$

where $d_{\min\text{QPSK}}$ is the minimum distance of the QPSK constellation.

Assuming that we use the RA scheme with Alamouti, the minimum distance of the received 16-QAM constellation is given by

$$(d_{\min}^2)_{\text{RA-Alam}} = \frac{\alpha^2 d_{\min\text{QPSK}}^2}{4} \left(|h_{ru,l1}|^2 + |h_{ru,(3-l)1}|^2 \right). \quad (5)$$

Let ρ be the ratio between the minimum and maximum of the channel power gains, that is,

$$\rho = \frac{\min \left(|h_{ru,l1,k}|^2, |h_{ru,(3-l)1,k}|^2 \right)}{\max \left(|h_{ru,l1,k}|^2, |h_{ru,(3-l)1,k}|^2 \right)}. \quad (6)$$

Then, when the channel power gains exhibit an asymmetry with ratio ρ , the asymptotic channel coding power gain of the proposed scheme, relative to the distributed Alamouti, is given by

$$G = 10 \log \left(\frac{1 + 4\rho}{1 + \rho} \right). \quad (7)$$

Therefore, the proposed scheme asymptotically achieves the performance of QPSK, in the case of high SNR and when the channels have equal average power gain, that is, an improvement of 4 dB relatively to 16-QAM; taking ρ into

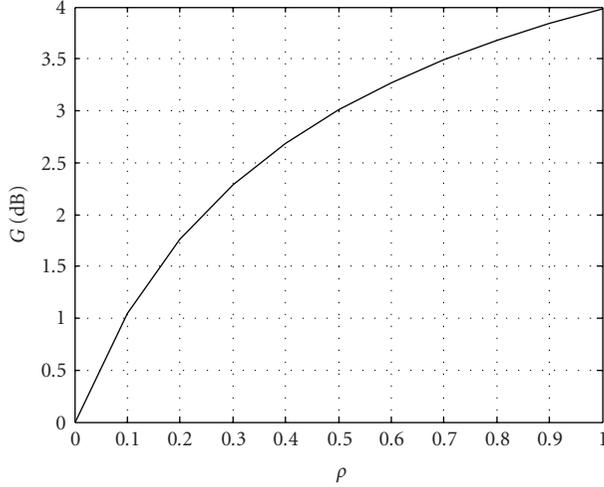


FIGURE 6: Coding gain obtained with RA Precoded in relation to RA Alamouti, for $K \times 1 \times 1$ system.

0, the performance will be that of distributed Alamouti, as we have only one path, reducing to a 16-QAM demodulation situation.

The gain as a function of the channel power gains ratio is represented in Figure 6.

The trellis code of the proposed scheme is represented in Figure 7. According to (1), we have defined four states, $u_k \in U$, $U = \{(0,0); (1,0); (0,1); (1,1)\}$, which are basically the QPSK symbols, whereas the transmitted QPSK symbols x_k are simply the scaled bipolar versions of u_k , so that they have the required power.

The weight associated with a state transition from u_{k-1} to u_k is defined as $\lambda_{k-1}(u_{k-1}, u_k)$. As we have alternate transmission through RN₁ and RN₂, the weights depend on the instant k and are given by

$$\lambda_{k-1}(u_{k-1}, u_k) = \alpha h_{ru,l,k} \left(\check{u}_{k-1} + \frac{1}{2} \check{u}_k \right), \quad (8)$$

with $l = 1$ if k is even and $l = 2$ if k is odd; \check{u}_k represents the QPSK soft-symbol associated with u_k , that is,

$$\check{u}_k = \sqrt{2} \left[u_k(1) + j u_k(2) - \frac{1+j}{2} \right]. \quad (9)$$

For each state, there are 4 branches arriving at each symbol. The Viterbi algorithm is then used to find the most probable sequence [18], with the Euclidian-squared distance given by

$$\nu(u_k, u_{k+1}) = |y_k - \lambda_k(u_k, u_{k+1})|^2. \quad (10)$$

3.2. RA Scheme with 2 Antennas at Relays. For the case of RNs being equipped with 2 antennas ($M = 2$), the signals transmitted in each relay are encoded in space-frequency

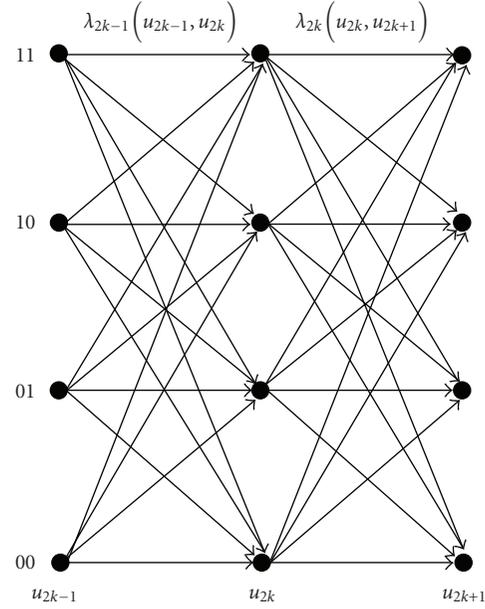


FIGURE 7: Trellis code for precoded algorithm.

using Alamouti code. The received signals at UT, in time slot k , for adjacent subcarrier p and $p + 1$, are given by

$$\begin{aligned} y_k^p &= \frac{1}{\sqrt{2}} \left(s_{k-1}^p h_{ru,l1,k}^p - s_{k-1}^{p+1*} h_{ru,l2,k}^p \right) + n_k^p, \\ y_k^{p+1} &= \frac{1}{\sqrt{2}} \left(s_{k-1}^{p+1} h_{ru,l1,k}^p + s_{k-1}^{p*} h_{ru,l2,k}^p \right) + n_k^{p+1}, \end{aligned} \quad (11)$$

with $l = 1$ in odd time slots and $l = 2$ in even time slots, where $h_{ru,l,m,k}^p$ represents the complex flat-fading cooperative Rayleigh channel of the m th antenna of RN₁ and UT, on time slot k and p th subcarrier position. Channels are considered flat for adjacent subcarriers; that is, the subcarrier separation is significantly lower than the coherence bandwidth of the channel.

At the UT, the SFBC decoding is performed, using coefficients $g_{lm,k}^p = \sqrt{2} h_{ru,l,m,k}^p$, as follows:

$$\begin{aligned} \hat{y}_k^p &= g_{1,k}^{p*} y_k^p + g_{2,k}^p y_k^{p+1*}, \\ \hat{y}_k^{p+1} &= -g_{2,k}^p y_k^{p*} + g_{1,k}^{p*} y_k^{p+1}. \end{aligned} \quad (12)$$

The obtained decoded symbols, expressed as

$$\begin{aligned} \hat{y}_k^p &= \alpha \left(|h_{ru,l1,k}^p|^2 + |h_{ru,l2,k}^p|^2 \right) \left(x_{k-1}^p + \frac{1}{2} x_k^p \right) \\ &+ \sqrt{2} \left(n_k^p h_{ru,l1,k}^{p*} + n_k^{p+1*} h_{ru,l2,k}^p \right), \end{aligned} \quad (13)$$

are then object of Viterbi decoding used to find the most probable sequence, similarly to the previous scheme, with the corresponding trellis code weights for time slot k given by (14), and with \check{u}_k represented in (9):

$$\lambda_k^p(u_k^p, u_k^{p+1}) = \alpha \left(|h_{ru,l1,k}^p|^2 + |h_{ru,l2,k}^p|^2 \right) \left(\check{u}_k^p + \frac{1}{2} \check{u}_k^{p+1} \right). \quad (14)$$

3.3. Error Probability and Diversity Gain Analysis. Let us compute the probability of an error event as shown in Figure 5, that is, assuming that the transmitted symbols correspond to the all-zero path, the probability that in decoding an incorrect path is taken at time k and remerges at time $k + 2$. This represents a lower bound on the actual probability of error, which is accurate for medium to high SNRs. Dropping for simplicity the subscripts ru, m, k in $h_{ru,lm,k}$ and assuming without loss of generality $h_1 \geq h_2$, the minimum distance between the two segments is given by

$$d_{\min}^2 = \alpha^2 d_{\min\text{QPSK}}^2 \left(\frac{|h_1|^2}{4 + |h_2|^2} \right), \quad (15)$$

where $d_{\min\text{QPSK}} = 2\sqrt{E_b}$ is the minimum distance for QPSK modulation.

The PEP for general QPSK modulation and coherent detection [22], under perfect synchronization, is given by

$$P_e = \frac{1}{2} \operatorname{erfc} \left(\frac{d_{\min}}{2\sqrt{N_0}} \right), \quad (16)$$

where $\operatorname{erfc}(z) = 2/\sqrt{\pi} \int_z^{+\infty} e^{-u^2} du$ is the complementary error function.

Replacing in (16) d_{\min} by the expression in (15), we obtain the conditioned error probability for $M = 1$:

$$\begin{aligned} P_{e|h_1, h_2} &= \frac{1}{2} \operatorname{erfc} \left(\sqrt{\frac{\alpha^2 E_b (|h_1|^2/4 + |h_2|^2)}{N_0}} \right) \\ &= \frac{1}{2} \operatorname{erfc}(\sqrt{\nu_1 + \nu_2}), \end{aligned} \quad (17)$$

where $\nu_1 = |h_1|^2 \gamma/4$, $\nu_2 = |h_2|^2 \gamma$, and $\gamma = \alpha^2 E_b/N_0$. The variables ν_i are i.i.d. and follow an exponential distribution with means $\bar{\nu}_1 = \gamma/4$ and $\bar{\nu}_2 = \gamma$ and the respective probability density function (pdf) is

$$f_{\nu_i}(\nu_i) = \begin{cases} \frac{1}{\bar{\nu}_i} e^{-\nu_i/\bar{\nu}_i}, & \nu_i \geq 0, \\ 0, & \nu_i < 0. \end{cases} \quad (18)$$

For the proposed scheme we then get the unconditioned probability of error as the following expression:

$$P_e = \frac{1}{2} \int_0^{+\infty} \int_0^{+\infty} \operatorname{erfc}(\sqrt{\nu_1 + \nu_2}) f_{\nu_1}(\nu_1) f_{\nu_2}(\nu_2) d\nu_1 d\nu_2, \quad (19)$$

which, by replacing the pdf expressions of ν_1 and ν_2 in (19), can be simplified to

$$P_e = \frac{2}{\gamma^2} \int_0^{+\infty} \int_0^{+\infty} \operatorname{erfc}(\sqrt{\nu_1 + \nu_2}) e^{-4\nu_1 + \nu_2/\gamma} d\nu_1 d\nu_2. \quad (20)$$

Integrating the previous equation, the final expression for PEP of the proposed scheme is extracted:

$$\begin{aligned} P_e &= \frac{1}{2\gamma} \left(\gamma - \gamma \sqrt{\frac{\gamma}{1+\gamma}} - \sqrt{\frac{\gamma}{4+\gamma}} \left(\frac{\gamma\sqrt{4+\gamma}}{3\sqrt{1+\gamma}} - \frac{1}{3} \right) \right) \\ &= \frac{1}{2} \left(1 - \frac{4}{3} \sqrt{\frac{\gamma}{1+\gamma}} + \frac{1}{3} \sqrt{\frac{\gamma}{4+\gamma}} \right). \end{aligned} \quad (21)$$

Expressing the error probability expression as a function of $x = \gamma^{-1}$, a simplified form is obtained:

$$P_e = \frac{1}{2} - \frac{2}{3}(1+x)^{-1/2} + \frac{1}{6}(1+4x)^{-1/2}. \quad (22)$$

Expanding this expression as a Mac-Laurin series up to order 2, (22) reduces to

$$P_e = \frac{3}{4}x^2 + r_2(x), \quad (23)$$

where $r_2(x)$ is the remainder term of order 2 [23].

For the high SNR regime, that is, for $\gamma \rightarrow \infty$, we obtain an approximated expression for the proposed error probability:

$$P_e \approx \frac{3}{4}\gamma^{-2}. \quad (24)$$

Diversity order, which is an important measure that we ultimately also need to keep track of, has been defined as the absolute values of the slopes of the error probability curve plotted on a log-log scale in high SNR regime [24]. From (24) we can see that the error probability decays as γ^{-2} , which means that our scheme achieves diversity order of 2.

4. Numerical Results

4.1. Assumptions and Conditions. Some assumptions were considered for this work, such as perfect CSI at the relays and at the UT, the transmitted power per time slot normalized to 1, and the distance between antenna elements of each BS and RNs large enough to assume uncorrelated antenna propagation channels. The block length used in the simulations, N , is of 3600 symbols.

In order to characterize propagation aspects as a whole, including the effects of path loss, shadowing, scattering, and others, we considered different link quality combinations, quantifying it in terms of SNR, given by the ratio between the link's received power and noise power. We define different SNRs for the second-hop cooperative links: $\text{RN}_1 \rightarrow \text{UT}$ and $\text{RN}_2 \rightarrow \text{UT}$, referred to as SNR_{c1} and SNR_{c2} , respectively; and for the direct link (the alternative link between the BS and the UT of the non-cooperative systems) as SNR_d . For simplicity and also assuming that the relays only forward BS data if decoding is correct, we do not refer to SNR differences in the first cooperative hop.

Three propagation scenarios were accounted for, differing on those links' SNRs, as shown in Figure 8. In Scenario 1 we assume that all the links have the same quality conditions, that is, $\text{SNR}_d = \text{SNR}_{c1} = \text{SNR}_{c2}$. We also include scenarios where the cooperative links, that is, $\text{RN}_1 \rightarrow \text{UT}$ and $\text{RN}_2 \rightarrow \text{UT}$, have higher quality than the direct link. The choice of these scenarios derives from the fact that, in most real situations, the cooperative link has higher transmission quality conditions than the worse alternative direct link, since selection of relay nodes takes the transmission quality of both cooperative hops into account. We then define Scenario 2 where the link between RN_1 and UT has an SNR 10 dB higher than the other two links, that is, $\text{SNR}_d = \text{SNR}_{c2}$

	SNR_d	SNR_{c1}	SNR_{c2}
Scenario 1	SNR_d	SNR_d	SNR_d
Scenario 2	SNR_d	$\text{SNR}_d + 10 \text{ dB}$	SNR_d
Scenario 3	SNR_d	$\text{SNR}_d + 10 \text{ dB}$	$\text{SNR}_d + 10 \text{ dB}$

FIGURE 8: Propagation scenarios considered for Monte Carlo simulations.

and $\text{SNR}_{c1} = \text{SNR}_d + 10 \text{ dB}$. Scenario 3 is our best quality cooperative scenario, where the entire cooperative path has better transmission quality conditions than the direct path, that is, $\text{SNR}_{c1} = \text{SNR}_{c2} = \text{SNR}_d + 10 \text{ dB}$.

In all considered systems, two information bits are transmitted per symbol interval, and thus all of them have the same spectral efficiency. We considered that the BS is equipped with 2 or 4 antennas for the non-cooperative systems. In systems where a space-frequency code is needed for 2 transmitting antennas, the well-known Alamouti coding is implemented [19]. In systems with 4 antennas transmitting simultaneously, we implement the QO-SFBC code proposed by Tirkkonen, Boariu, and Hottinen (TBH) in [20].

The schemes considered in our evaluations are presented next, where the former bullet includes the proposed ones and the two last ones are used as references:

- (i) hereby proposed scheme, with precoded QPSK and Viterbi algorithm decoding, for 2 relays with 1 and 2 antennas (RA-Precoded $K \times 1 \times 1$ and RA-Precoded $K \times 2 \times 1$, resp.);
- (ii) distributed SFBC for 2 relays with 1 and 2 antennas using 16-QAM modulation (RA Alamouti $K \times 1 \times 1$ and RA TBH $K \times 2 \times 1$, resp.);
- (iii) non-cooperative 4×1 QPSK with QO-SFBC code with a continuous link available (Non-coop TBH 4×1);
- (iv) non-cooperative 2×1 QPSK Alamouti coding with a continuous link available (Non-coop Alamouti 2×1).

The results of the cooperative and non-cooperative schemes are presented in terms of bit error rate (BER) as a function of E_b/N_0 of the direct link used for reference, where E_b is the received energy per bit at the UT and $N_0/2$ is the bilateral noise power spectral density.

4.2. PEP Analysis Validation. The analytical PEP derivation is corroborated by the BER performance obtained through Monte Carlo simulations, for the RA scheme with 1 antenna in each relay, assuming error-free transmission between BS and the RNs. Theoretical and simulated BER curves are shown in Figure 9, including the theoretical upper bound derived previously for high SNR regime. The simulation curve has approximately the same behaviour as that of the lower bound provided in (21), only differing for low SNRs. In real situations and at low SNRs, error events may correspond to paths that are not corresponding to the minimum distance, which results in the differences between

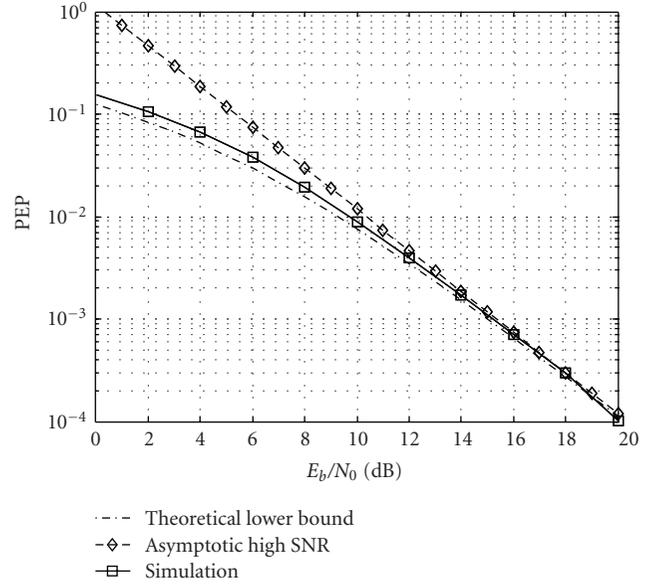


FIGURE 9: Theoretical and simulated error probability for RA-Precoded scheme with $M = 1$.

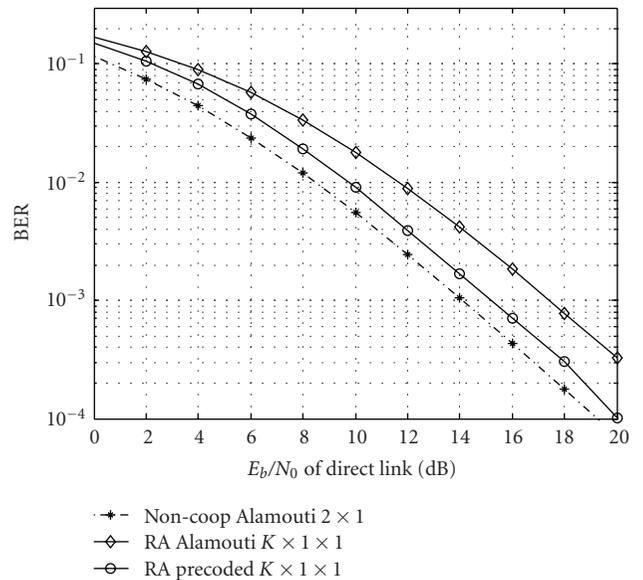


FIGURE 10: BER of cooperative systems with 1 antenna per relay and of reference systems for Scenario 1.

the lower bound and simulated curves. These are anyhow lower than 1 dB and negligible for $E_b/N_0 \geq 12 \text{ dB}$. We can also observe that the simulated curve has the same linear decay as the asymptotic curve given by (24) for high SNRs, confirming the diversity order of 2.

4.3. Scheme with 1 Antenna in Each Relay. Cooperative and reference systems performances for the case of 1 antenna in each relay ($M = 1$) are shown in Figure 10 for Scenario 1. In this case, the reference systems presented are the non-cooperative Alamouti 2×1 and RA Alamouti $K \times 1 \times 1$ ones.

When comparing the RA-Precoded scheme against RA Alamouti, we observe an improvement of 2.2 dB, for BER = 10^{-3} . This, in turn, derives from the precoding used in the proposed scheme, which mitigates some of the penalty resultant from the half-duplex constraint at the relays, avoiding the use of a higher modulation order.

The proposed cooperative scheme has a penalty of about 1 dB from the best reference, that is, 2×1 QPSK Alamouti coding with a continuous link available, for the same BER conditions. It is however worthwhile to point out that in our reference we assume independence between the channels. In practice using colocated antennas inevitably leads to some correlation between the channels, in fact reducing such 1 dB of penalty, or even outperforming it in the case of high correlation.

In Figure 11, the performance of the same schemes in Scenario 2 is presented. In this scenario conditions the proposed precoded scheme outperform the equivalent non-cooperative system. Improvements of 4 dB are obtained in comparison with 2×1 Alamouti, for BER = 10^{-3} . However, the RA Alamouti scheme is still worse than the non-cooperative scheme with 2 antennas in BS. The coding gain between the precoded scheme and the RA Alamouti is of 6 dB for the same BER conditions, which is higher than that in the previous scenario.

In Figure 12, both links between relays and UT have SNRs 10 dB higher than the direct link (Scenario 3). In this case, the cooperative schemes have the same resulting behaviour as in the previous scenarios, although the cooperative schemes achieve better performances, as expected. The difference between non-cooperative 2×1 and the RA Precoded schemes is now more than 8 dB, for BER = 10^{-3} (for best visualisation purposes, the non-cooperative 2×1 curve is not completely shown in the plot).

Comparing with the distributed RA Alamouti, we have an improvement of about 2.2 dB in using the proposed code, for BER = 10^{-3} , which is the same difference than in Scenario 1.

4.4. Scheme with 2 Antennas in Each Relay. For the scheme with 2 antennas in RNs ($M = 2$), the same study was made, for the same scenarios. In this case, the chosen reference systems are the non-cooperative Alamouti 2×1 and TBH 4×1 systems and the RA scheme with the TBH code applied to the relay nodes.

In Figure 13, all the links have the same transmission conditions. In this scenario case, higher coding gains are obtained with the proposed algorithm than those in Figure 10, as expected, since we have now 2 antennas in each relay. An enhancement of about 4 dB is achieved with the RA Precoded scheme, compared with the cooperative scheme using TBH code, for BER = 10^{-3} . Comparing with the non-cooperative systems, the proposed scheme outperforms the non-cooperative system 2×1 by about 2 dB, for the same BER. The performance of the new algorithm also overpasses the non-cooperative system 4×1 for high SNRs, specifically for $E_b/N_0 > 12$ dB. This happens because, oppositely to the

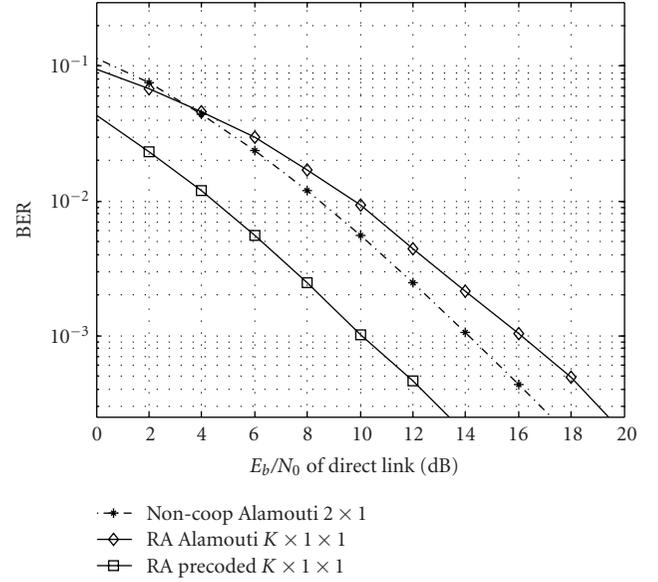


FIGURE 11: BER of cooperative systems with 1 antenna per relay and of reference systems for Scenario 2.

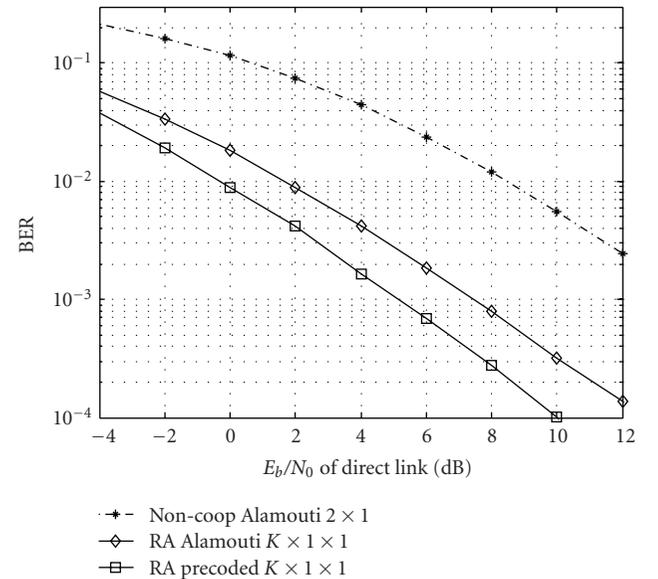


FIGURE 12: BER of cooperative systems with 1 antenna per relay and of reference systems for Scenario 3.

Alamouti coding, space-time codes for 4 antennas are not fully orthogonal, not achieving full diversity.

For Scenario 2 (results in Figure 14), as expected, the difference between the RA and non-cooperative systems is higher than that in the previous scenario. The RA-Precoded scheme has improvements of 6.2 dB and more than 15 dB in comparison with the non-cooperative 2×1 and 4×1 systems, respectively, for BER = 10^{-3} . As in the RA $K \times 1 \times 1$, the difference between the algorithms used in cooperative schemes is higher than that in the first scenario, differing by about 7.5 dB, for BER = 10^{-3} .

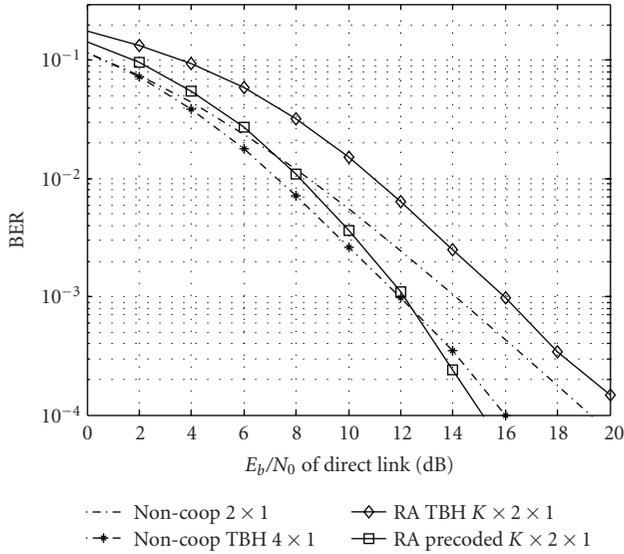


FIGURE 13: BER of cooperative systems with 2 antennas per relay and of reference systems for Scenario 1.

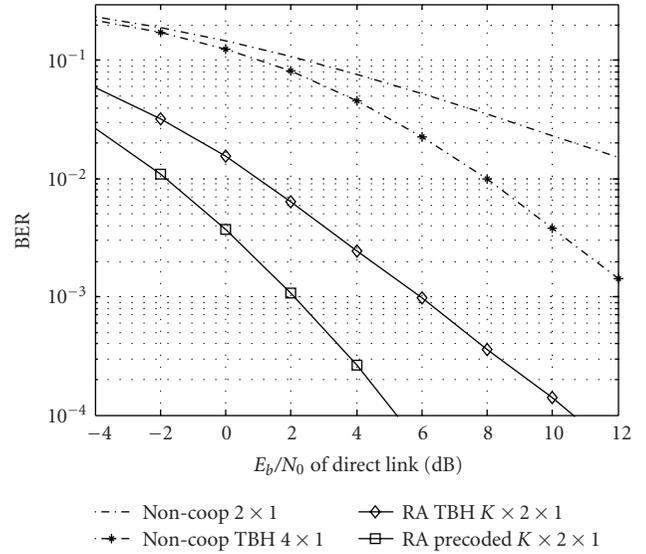


FIGURE 15: BER of cooperative systems with 2 antennas per relay and of reference systems for Scenario 3.

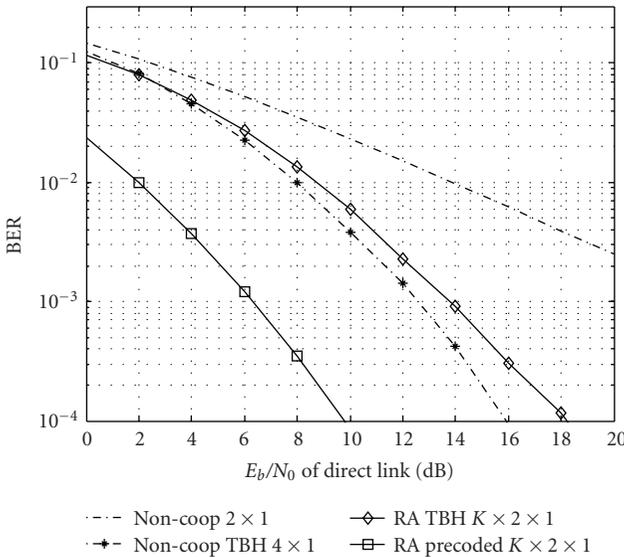


FIGURE 14: BER of cooperative systems with 2 antennas per relay and of reference systems for Scenario 2.

For Scenario 3 (in Figure 15), even higher coding gains are obtained with cooperative systems, in comparison with the non-cooperative ones. For example, the proposed algorithm in comparison with the equivalent non-cooperative 4×1 system has a gain higher than 10 dB. The difference between both RA schemes is similar to the one in Scenario 1.

5. Conclusions

We proposed a novel data-precoded relay-assisted scheme, which ensures spatial diversity for cooperative systems with 2 relays, while ensuring spectral efficiency. Numerical results

for the precoded scheme were computed, in scenarios with different link quality conditions, for the cases of each relay node being equipped with either 1 or 2 antennas.

The implemented precoding mitigates some of the penalty resulting from the half-duplex constraint at the relays. It brings the performance very close to the one achieved when a direct continuous link is available and SFBC coding is used at the BS. Actually, for the case of 2 antennas in each relay, the precoded scheme outperforms the non-cooperative one for high SNR regime, due to the non-orthogonality of space-frequency codes for 4 transmitting antennas. Improvements are obtained for scenarios where cooperative links have higher quality than the direct link, being more pronounced as the quality of the cooperative links increases.

We observe that, independently of the propagation scenario, both precoded schemes outperform the equivalent distributed SFBC cooperative schemes, achieving better performance due to the coding gain obtained with precoding. Even for the most probable situation of asymmetric quality conditions between cooperative links, results show that the proposed scheme is better than the reference cooperative ones. In these cases, the difference between the 2 cooperative schemes is higher. For example, it is of about 7.5 dB for $\text{BER} = 10^{-3}$, considering the case of $M = 2$.

We also observe that the extra antenna in each relay leads to a considerable improvement in the overall system performance, which is at least of 3 dB for $\text{BER} = 10^{-3}$. Furthermore, the performance difference between the precoded schemes and the respective equivalent distributed SFBC schemes are higher for the case of having 2 antennas in each relay.

From the presented results, it is clear that the proposed cooperative schemes can be used to extend the coverage mainly in scenarios where the quality of the direct link is poor, as is the case of cluttered urban environments.

Acknowledgments

The work presented in this paper was supported by the European project CODIV, Portuguese projects CADWIN and AGILE, and by the Portuguese Foundation for Science and Technology (FCT) with a grant for the first author.

References

- [1] G. J. Foschini and M. J. Gans, "On limits of wireless communications in a fading environment when using multiple antennas," *Wireless Personal Communications*, vol. 6, no. 3, pp. 311–335, 1998.
- [2] F. H. P. Fitzek and M. D. Katz, *Cooperation in Wireless Networks: Principles and Applications*, Springer, Dordrecht, The Netherlands, 2006.
- [3] M. Dohler, *Virtual antenna arrays*, Ph.D. thesis, King's College London, London, UK, November 2003.
- [4] A. Sendonaris, E. Erkip, and B. Aazhang, "User cooperation diversity—part I: system description," *IEEE Transactions on Communications*, vol. 51, no. 11, pp. 1927–1938, 2003.
- [5] J. N. Laneman, D. N. C. Tse, and G. W. Wornell, "Cooperative diversity in wireless networks: efficient protocols and outage behavior," *IEEE Transactions on Information Theory*, vol. 50, no. 12, pp. 3062–3080, 2004.
- [6] M. Yuksel and E. Erkip, "Diversity-multiplexing tradeoff in multiple-antenna relay systems," in *Proceedings of IEEE International Symposium on Information Theory (ISIT '06)*, pp. 1154–1158, Seattle, Wash, USA, July 2006.
- [7] H. Muhaidat and M. Uysal, "Cooperative diversity with multiple-antenna nodes in fading relay channels," *IEEE Transactions on Wireless Communications*, vol. 7, no. 8, pp. 3036–3046, 2008.
- [8] K. J. R. Liu, A. K. Sadek, W. Su, and A. Kwasinski, *Cooperative Communications and Networking*, Cambridge University Press, New York, NY, USA, 2009.
- [9] Y. Jing and B. Hassibi, "Distributed space-time coding in wireless relay networks," *IEEE Transactions on Wireless Communications*, vol. 5, no. 12, pp. 3524–3536, 2006.
- [10] Z. Yi and I. M. Kim, "Single-symbol ML decodable distributed STBCs for cooperative networks," *IEEE Transactions on Information Theory*, vol. 53, no. 8, pp. 2977–2985, 2007.
- [11] D. Sreedhar, A. Chockalingam, and B. Sundar Rajan, "Single-symbol ML decodable distributed STBCs for partially-coherent cooperative networks," in *Proceedings of IEEE International Symposium on Information Theory (ISIT '08)*, pp. 2672–2681, Toronto, Canada, July 2008.
- [12] J. Harshan and B. S. Rajan, "High-rate, single-symbol ML decodable precoded DSTBCs for cooperative networks," *IEEE Transactions on Information Theory*, vol. 55, no. 5, pp. 2004–2015, 2009.
- [13] G. S. Rajan and B. S. Rajan, "A non-orthogonal distributed space-time coded protocol—part I: signal model and design criteria," in *Proceedings of IEEE Information Theory Workshop (ITW '06)*, pp. 385–389, Chengdu, China, October 2006.
- [14] G. M. Kraidy, N. Gresset, and J. J. Boutros, "Coding for the non-orthogonal amplify-and-forward cooperative channel," in *Proceedings of the IEEE Information Theory Workshop (ITW '07)*, pp. 626–631, Lake Tahoe, Calif, USA, September 2007.
- [15] X. Tang and Y. Hua, "Optimal design of non-regenerative MIMO wireless relays," *IEEE Transactions on Wireless Communications*, vol. 6, no. 4, pp. 1398–1406, 2007.
- [16] B. K. Chalise and L. Vandendorpe, "MIMO relay design for multipoint-to-multipoint communications with imperfect channel state information," *IEEE Transactions on Signal Processing*, vol. 57, no. 7, pp. 2785–2796, 2009.
- [17] S. Teodoro, A. Silva, J. M. Gil, and A. Gameiro, "Virtual MIMO schemes for downlink space-frequency coding OFDM systems," in *Proceedings of the 20th IEEE Personal, Indoor and Mobile Radio Communications Symposium (PIMRC '09)*, Tokyo, Japan, September 2009.
- [18] A. J. Viterbi, "Error bounds on convolutional codes and an asymptotically optimum decoding algorithms," *IEEE Transactions on Information Theory*, vol. 13, no. 2, pp. 260–269, 1967.
- [19] S. M. Alamouti, "A simple transmit diversity technique for wireless communications," *IEEE Journal on Selected Areas in Communications*, vol. 16, no. 8, pp. 1451–1458, 1998.
- [20] O. Tirkkonen, A. Boariu, and A. Hottinen, "Minimal non-orthogonality rate 1 space-time block code for 3+ Tx antennas," in *Proceedings of the 6th IEEE International Symposium on Spread Spectrum Techniques and Applications (ISSSTA '00)*, pp. 429–432, Parsippany, NJ, USA, September 2000.
- [21] S. Teodoro, A. Silva, J. M. Gil, and A. Gameiro, "Distributed space-time code using precoding for cellular systems," in *Proceedings of the 72nd IEEE Vehicular Technology Conference (VTC '10)*, Ottawa, Canada, September 2010.
- [22] A. Goldsmith, *Wireless Communications*, Cambridge University Press, New York, NY, USA, 2005.
- [23] G. James, D. Burley, P. Dyke, J. Searl, D. Clements, and J. Wright, *Modern Engineering Mathematics*, Prentice-Hall, Harlow, UK, 3rd edition, 2001.
- [24] M. K. Simon and M. S. Alouini, *Digital Communication over Fading Channels*, Wiley-Interscience, New York, NY, USA, 2nd edition, 2005.



Preliminary call for papers

The 2011 European Signal Processing Conference (EUSIPCO-2011) is the nineteenth in a series of conferences promoted by the European Association for Signal Processing (EURASIP, www.urasip.org). This year edition will take place in Barcelona, capital city of Catalonia (Spain), and will be jointly organized by the Centre Tecnològic de Telecomunicacions de Catalunya (CTTC) and the Universitat Politècnica de Catalunya (UPC).

EUSIPCO-2011 will focus on key aspects of signal processing theory and applications as listed below. Acceptance of submissions will be based on quality, relevance and originality. Accepted papers will be published in the EUSIPCO proceedings and presented during the conference. Paper submissions, proposals for tutorials and proposals for special sessions are invited in, but not limited to, the following areas of interest.

Areas of Interest

- Audio and electro-acoustics.
- Design, implementation, and applications of signal processing systems.
- Multimedia signal processing and coding.
- Image and multidimensional signal processing.
- Signal detection and estimation.
- Sensor array and multi-channel signal processing.
- Sensor fusion in networked systems.
- Signal processing for communications.
- Medical imaging and image analysis.
- Non-stationary, non-linear and non-Gaussian signal processing.

Submissions

Procedures to submit a paper and proposals for special sessions and tutorials will be detailed at www.eusipco2011.org. Submitted papers must be camera-ready, no more than 5 pages long, and conforming to the standard specified on the EUSIPCO 2011 web site. First authors who are registered students can participate in the best student paper competition.

Important Deadlines:



Proposals for special sessions	15 Dec 2010
Proposals for tutorials	18 Feb 2011
Electronic submission of full papers	21 Feb 2011
Notification of acceptance	23 May 2011
Submission of camera-ready papers	6 Jun 2011

Webpage: www.eusipco2011.org

Organizing Committee

Honorary Chair

Miguel A. Lagunas (CTTC)

General Chair

Ana I. Pérez-Neira (UPC)

General Vice-Chair

Carles Antón-Haro (CTTC)

Technical Program Chair

Xavier Mestre (CTTC)

Technical Program Co-Chairs

Javier Hernando (UPC)
Montserrat Pardàs (UPC)

Plenary Talks

Ferran Marqués (UPC)
Yonina Eldar (Technion)

Special Sessions

Ignacio Santamaría (Universidad de Cantabria)
Mats Bengtsson (KTH)

Finances

Montserrat Najar (UPC)

Tutorials

Daniel P. Palomar (Hong Kong UST)
Beatrice Pesquet-Popescu (ENST)

Publicity

Stephan Pfletschinger (CTTC)
Mònica Navarro (CTTC)

Publications

Antonio Pascual (UPC)
Carles Fernández (CTTC)

Industrial Liaison & Exhibits

Angeliki Alexiou (University of Piraeus)
Albert Sitjà (CTTC)

International Liaison

Ju Liu (Shandong University-China)
Jinhong Yuan (UNSW-Australia)
Tamas Sziranyi (SZTAKI -Hungary)
Rich Stern (CMU-USA)
Ricardo L. de Queiroz (UNB-Brazil)

